

ANALYSIS OF SCATTERING WITH MULTI-SLOTTED CYLINDER WITH THICKNESS: TM CASE

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Abstract—An exact series solution for radiation and scattering of the dielectric-loaded multi-slotted cylinder with thickness is formulated by using radial mode matching technique. The radiated and guided fields are represented in terms of an infinite series of radial modes. By applying the appropriate boundary conditions, the coefficients of radiated and guided fields are obtained. The behaviors of resonance features are characterized for variation in frequencies, source positions, slot thickness, and dielectric coating properties.

1. INTRODUCTION

A shield is the layer of conducting material which partially or completely envelops an electric circuit. It therefore affects the amount of electromagnetic radiation penetrating into the electric circuit from the external environment as well as the electromagnetic energy escaping from the electric circuit to the external environment. A variety of materials are used for shielding with a wide range of electrical conductivity, permittivity, magnetic permeability, and thickness. Shields invariably contain openings (apertures) for accessing and cooling and a number of joints and seams through which electromagnetic radiation can penetrate. When the envelope is slotted, environmental electromagnetic fields can create an important field inside the envelope, which can affect the electrical performance of the enclosed devices or circuits. In this case, the knowledge of the field distribution and polarization can help designers to choose the best layout and orientation for the most sensitive devices.

The slotted circular cylinder is one of the most investigated geometries in the area of scattering and radiation (Fig. 1). The

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circular slotted cylinder has become the subject of extensive study due to its engineering applications in devices such as aperture and leaky wave antennas, microstrip transmission lines, microstrip antennas, composite missiles, and engine tubes of jet aircraft. The E -polarization case has the received attention in the researches with various techniques such as an integral equation approach by Senior [1] and by an approximate analytical approach [2]. Hussein and Hamid [3] have discussed the problem of the scattering by a perfectly conducting circular cylinder, with an infinite axial slot. The solution was later extended to include the problems of a multi-slotted circular cylinder [4]. The theory of the characteristic modes of a slot/slots in a conducting cylinder and their use for penetration and scattering was given in [5, 6]. The slotted cylinder, which is coated with an absorbing material either from inside or from outside, has been analyzed using the dual series based Riemann-Hilbert problem (RHP) technique in [7, 8]. Circular cylindrical surfaces covered periodically with the metallic strips and patches are considered in [9] using dual-series technique and in [10] using mixed spectral domain method (SDM), conjugated gradient method (CGM) and fast Fourier transform (FFT).

Although the problem in determining the electromagnetic scattering from and penetration of conducting cylinders with axial slots has been investigated by many researchers with various techniques [11–29], the determination of the transmitted field through multi-slotted circular cylinder in a thick conducting shell covered with dielectrics has received little attention. A simplified model of the problem to be solved here is represented by Fig. 2 and Fig. 3, where an electric line current is placed inside or outside a thick conducting cylindrical shell having multiple slots filled with a dielectric. The source produces an electromagnetic wave with its electric field vector parallel to the axis of the shell.

In this paper, an exact series solution for transmission and shielding effects of an electric line current placed inside or outside the multi-slotted circular cylinder in a thick conducting shell is developed for the first time by using a radial mode matching technique.

2. FORMULATION OF ELECTRICAL LINE CURRENT PLACED INSIDE

Consider an electric line current source inside the shell (ρ_i, ϕ_i) illuminating dielectric-coated multi-slotted circular cylinder with N th slot, as shown in Fig. 2. Throughout the work, $e^{j\omega t}$ time harmonic factor is suppressed. In region (I) ($\rho < a, k_o$), the total electric field can be represented as the sum of electric field of a line current and



Figure 1. Geometry of a single slotted circular cylinder, multi-slotted circular cylinder and concentrically loaded slotted circular cylinder.

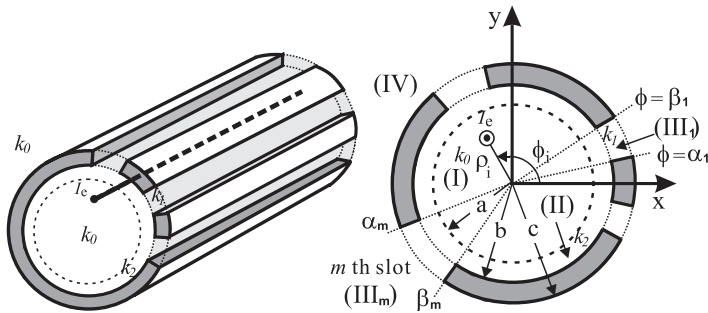


Figure 2. Geometry of an electrical line current placed inside a dielectric-loaded multi-slotted circular cylinder.

diffracted field, i.e.,

$$E_z^I(\rho, \phi) = E_o^I \begin{cases} \sum_{n=-\infty}^{\infty} \left\{ H_n^{(2)}(k_o \rho_i) J_n(k_o \rho) e^{-jn\phi_i} + D_n J_n(k_o \rho) \right\} e^{jn\phi}, & \rho < \rho_i \\ \sum_{n=-\infty}^{\infty} \left\{ J_n(k_o \rho_i) H_n^{(2)}(k_o \rho) e^{-jn\phi_i} + D_n J_n(k_o \rho) \right\} e^{jn\phi}, & \rho_i < \rho < a \end{cases} \quad (1)$$

where $E_o^I = -\eta_o k_o I_e / 4$, η_o is the free space intrinsic impedance and I_e is the strength of the electric current filament, k_o is the free space wave number and $J_n(\dots)$ and $H_n^{(2)}(\dots)$ are Bessel function of the first kind and Hankel function of the second kind, respectively. In region (II) ($a < \rho < b$, k_2), the electric field inside the dielectric coating can

be represented as

$$E_z^{II}(\rho, \phi) = E_o^l \sum_{n=-\infty}^{\infty} \left\{ J_n(k_o \rho_i) G_n(k_2 \rho) e^{-jn\phi_i} + D_n F_n(k_2 \rho) \right\} e^{jn\phi} \quad (2)$$

where

$$\begin{aligned} G_n(k_2 \rho) &= \frac{1}{2} \pi k_2 a \left\{ H Y_n J_n(k_2 \rho) - H J_n Y_n(k_2 \rho) \right\} \\ F_n(k_2 \rho) &= \frac{1}{2} \pi k_2 a \left\{ J Y_n J_n(k_2 \rho) - J J_n Y_n(k_2 \rho) \right\} \\ H Y_n(k_o a) &= H_n^{(2)}(k_o a) Y_n'(k_2 a) - \frac{k_o}{k_2} H_n^{(2)'}(k_o a) Y_n(k_2 a) \\ H J_n(k_o a) &= H_n^{(2)}(k_o a) J_n'(k_2 a) - \frac{k_o}{k_2} H_n^{(2)'}(k_o a) J_n(k_2 a) \\ J Y_n &= J_n(k_o a) Y_n'(k_2 a) - \frac{k_o}{k_2} J_n'(k_o a) Y_n(k_2 a) \\ J J_n &= J_n(k_o a) J_n'(k_2 a) - \frac{k_o}{k_2} J_n'(k_o a) J_n(k_2 a). \end{aligned}$$

Here, k_o is the free space wave number and $k_2 = k_o \sqrt{\epsilon_{r2}}$ while $Y_n(\dots)$ is the Bessel function of the second kind. It is worth noting that the boundary conditions of the continuous tangential components of the electric and magnetic fields on the surface between the region (I) and region (II) are satisfied in Equation (2). The transmitted fields in the m th slot region (III_m) ($b < \rho < c$, $\alpha_m < \phi < \beta_m$, k_1) and region (IV) ($\rho > c$, k_o) can be expressed as follows

$$E_z^{III_m}(\rho, \phi) = E_o^l \sum_{p=1}^{\infty} \left\{ B_{p_m} J_{\mu_m}(k_1 \rho) + C_{p_m} Y_{\mu_m}(k_1 \rho) \right\} \sin \mu_m(\phi - \alpha_m) \quad (3)$$

$$E_z^{IV}(\rho, \phi) = E_o^l \sum_{n=-\infty}^{\infty} A_n H_n^{(2)}(k_o \rho) e^{jn\phi} \quad (4)$$

where $\mu_m = p_m \pi / \phi_m$, $\phi_m = \beta_m - \alpha_m$, $p = 1, 2, 3, \dots$, $m = 1, 2, \dots, N$ and $k_1 = k_o \sqrt{\epsilon_{r1}}$.

In order to determine the unknown coefficients A_n , B_{p_m} , C_{p_m} and D_n , the boundary conditions of the zero tangential electric field at the surface of conductor at $\rho = b$ and c and continuous fields (i.e., E_z and

H_ϕ) across the aperture ($\alpha_m < \phi < \beta_m$, $m = 1, 2, \dots, N$) are applied to obtain

$$B_{p_m} = -\frac{2}{\phi_m} \frac{Y'_{\mu_m}(k_1 b)}{\Delta_{\mu_m}} \frac{k_o}{k_1} \sum_{n=-\infty}^{\infty} A_n H_n^{(2)'}(k_o c) f_{n\mu}^m + \frac{2}{\phi_m} \frac{Y'_{\mu_m}(k_1 c)}{\Delta_{\mu_m}} \frac{k_2}{k_1} \sum_{n=-\infty}^{\infty} Z_n f_{n\mu}^m \quad (5)$$

$$C_{p_m} = \frac{2}{\phi_m} \frac{J'_{\mu_m}(k_1 b)}{\Delta_{\mu_m}} \frac{k_o}{k_1} \sum_{n=-\infty}^{\infty} A_n H_n^{(2)'}(k_o c) f_{n\mu}^m - \frac{2}{\phi_m} \frac{J'_{\mu_m}(k_1 c)}{\Delta_{\mu_m}} \frac{k_2}{k_1} \sum_{n=-\infty}^{\infty} Z_n f_{n\mu}^m \quad (6)$$

$$\sum_{n=-\infty}^{\infty} \sum_{m=1}^N A_n H_n^{(2)'}(k_o c) R_{kn}^m - \sum_{n=-\infty}^{\infty} \sum_{m=1}^N \left\{ \frac{F_n(k_2 b)}{F'_n(k_2 b)} \delta_{kn} - I_{kn}^m \right\} Z_n = J_k(k_o \rho_i) \left\{ G_k(k_2 b) - \frac{F_k(k_2 b)}{F'_k(k_2 b)} G'_k(k_2 b) \right\} e^{-jk\phi_i} \quad (7)$$

$$\sum_{n=-\infty}^{\infty} \sum_{m=1}^N \left\{ \delta_{kn} - \frac{H_n^{(2)'}(k_o c)}{H_n^{(2)}(k_o c)} Q_{kn}^m \right\} A_n H_n^{(2)}(k_o c) = \sum_{n=-\infty}^{\infty} \sum_{m=1}^N Z_n M_{kn}^m \quad (8)$$

where δ_{kn} is the Kronecker delta,

$$Z_n \equiv J_n(k_o \rho_i) G'_n(k_2 b) e^{-jn\phi_i} + D_n F'_n(k_2 b) \\ \Delta_{\mu_m} \equiv J'_{\mu_m}(k_1 b) Y'_{\mu_m}(k_1 c) - J'_{\mu_m}(k_1 c) Y'_{\mu_m}(k_1 b)$$

and

$$I_{kn}^m = \frac{1}{\pi \phi_m} \frac{k_2}{k_1} \sum_{p_m=1}^{\infty} \frac{J_{\mu_m}(k_1 b) Y'_{\mu_m}(k_1 c) - J'_{\mu_m}(k_1 c) Y_{\mu_m}(k_1 b)}{\Delta_{\mu_m}} f_{n\mu}^m \hat{f}_{k\mu}^m \\ R_{kn}^m = -\frac{2}{\pi^2 \phi_m} \frac{1}{k_1 b} \frac{k_o}{k_1} \sum_{p_m=1}^{\infty} \frac{f_{n\mu}^m \hat{f}_{k\mu}^m}{\Delta_{\mu_m}} \\ M_{kn}^m = \frac{2}{\pi^2 \phi_m} \frac{1}{k_1 c} \frac{k_2}{k_1} \sum_{p_m=1}^{\infty} \frac{f_{n\mu}^m \hat{f}_{k\mu}^m}{\Delta_{\mu_m}} \\ Q_{kn}^m = \frac{1}{\pi \phi_m} \frac{k_o}{k_1} \sum_{p_m=1}^{\infty} \frac{J'_{\mu_m}(k_1 b) Y_{\mu_m}(k_1 c) - J_{\mu_m}(k_1 c) Y'_{\mu_m}(k_1 b)}{\Delta_{\mu_m}} f_{n\mu}^m \hat{f}_{k\mu}^m$$

$$f_{n\mu}^m = \int_{\alpha_m}^{\beta_m} e^{jn\phi} \sin \mu_m(\phi - \alpha_m) d\phi$$

$$\hat{f}_{n\mu}^m = \int_{\alpha_m}^{\beta_m} e^{-jn\phi} \sin \mu_m(\phi - \alpha_m) d\phi.$$

Once the unknown coefficients A_n and D_n are determined from the simultaneous Equations (7) and (8), B_{p_m} and C_{p_m} can be evaluated by using the Equations (5) and (6).

3. FORMULATION OF ELECTRICAL LINE CURRENT PLACED OUTSIDE

Considering TM_z line source at (ρ_i, ϕ_i) illuminating dielectric-loaded multi-slotted cylinder with N th slot, as shown in Fig. 3. The total electric field in regin (IV) ($\rho > c, 0 < \phi < 2\pi, k_o$) can be represented by two parts: the incident and scattered fields as follows,

$$E_z^{IV}(\rho, \phi) = E_o^l \begin{cases} \sum_{n=-\infty}^{\infty} \left\{ s_n H_n^{(2)}(k_o \rho_i) J_n(k_o \rho) + A_n^o H_n^{(2)}(k_o \rho) \right\} e^{jn\phi}, & c < \rho < \rho_i \\ \sum_{n=-\infty}^{\infty} \left\{ s_n J_n(k_o \rho_i) H_n^{(2)}(k_o \rho) + A_n^o H_n^{(2)}(k_o \rho) \right\} e^{jn\phi}, & \rho > \rho_i \end{cases} \quad (9)$$

where $E_o^l = -\eta_o k_o I_e / 4$, $s_n = e^{-jn\phi_i}$. In regions (I) ($\rho < a, k_3$) and (II) ($a < \rho < b, k_2$), the transmitted field inside the dielectric cylinder

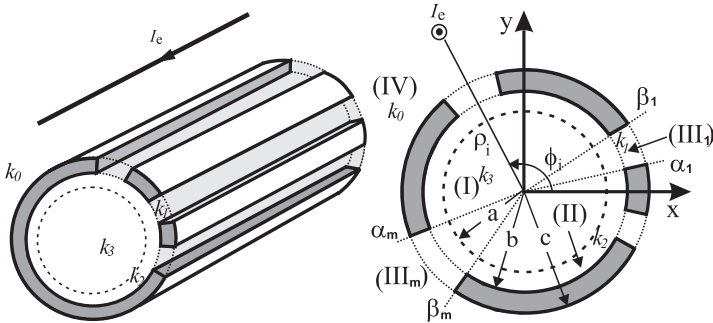


Figure 3. Geometry of an electrical line current placed outside the dielectric-loaded multi-slotted circular cylinder.

can be represented as

$$E_z^{II}(\rho, \phi) = E_o^l \sum_{n=-\infty}^{\infty} D_n^\circ F_n(k_2 \rho) e^{jn\phi} \quad (10)$$

$$E_z^I(\rho, \phi) = E_o^l \sum_{n=-\infty}^{\infty} D_n^\circ J_n(k_3 \rho) e^{jn\phi} \quad (11)$$

where

$$\begin{aligned} F_n(k_2 \rho) &= \frac{1}{2} \pi k_2 a \left\{ J Y_n J_n(k_2 \rho) - J J_n Y_n(k_2 \rho) \right\} \\ J Y_n &= J_n(k_1 a) Y_n'(k_2 a) - \frac{k_1}{k_2} J_n'(k_1 a) Y_n(k_2 a) \\ J J_n &= J_n(k_1 a) J_n'(k_2 a) - \frac{k_1}{k_2} J_n'(k_1 a) J_n(k_2 a) \end{aligned}$$

Assuming that region (I) is filled with the conducting core, the above equation can be expressed as follows

$$\begin{aligned} E_z^{II}(\rho, \phi) &= E_o^l \sum_{n=-\infty}^{\infty} D_n^\circ F_n(k_2 \rho) e^{jn\phi} \\ E_z^I(\rho, \phi) &= 0 \end{aligned}$$

where

$$F_n(k_2 \rho) = \frac{1}{2} \pi k_2 a \left\{ J_n(k_2 \rho) Y_n(k_2 a) - J_n(k_2 a) Y_n(k_2 \rho) \right\}$$

In the m th slot region (III_m) ($\alpha_m \leq \phi \leq \beta_m$, $b < \rho < c$, k_1), the total fields $E_z^{III_m}(\rho, \phi)$ can be represented as the summation of wedged-plate waveguide modes,

$$E_z^{III_m}(\rho, \phi) = E_o^l \sum_{p_m=1}^{\infty} \left\{ B_{p_m}^\circ J_{\mu_m}(k_1 \rho) + C_{p_m}^\circ Y_{\mu_m}(k_1 \rho) \right\} \sin \mu_m(\phi - \alpha_m) \quad (12)$$

To determine the unknown coefficients A_n° , $B_{p_m}^\circ$, $C_{p_m}^\circ$ and D_n° , the boundary conditions of the zero tangential electric field at the surface of conductor at $\rho = b$ and $\rho = c$ and continuous fields across the aperture ($\alpha_m < \phi < \beta_m$, $m = 1, 2, \dots, N$) are applied to obtain

$$\begin{aligned} B_{p_m}^\circ &= \frac{2}{\phi_m} \frac{Y_{\mu_m}'(k_1 c)}{\Delta_{\mu_m}} \frac{k_2}{k_1} \sum_{n=-\infty}^{\infty} D_n^\circ F_n'(k_2 b) f_{n\mu}^m - \frac{2}{\phi_m} \frac{Y_{\mu_m}'(k_1 b)}{\Delta_{\mu_m}} \frac{k_o}{k_1} \\ &\quad \sum_{n=-\infty}^{\infty} \left\{ s_n H_n^{(2)}(k_o \rho_i) J_n'(k_o c) + A_n^\circ H_n^{(2)'}(k_o c) \right\} f_{n\mu}^m \end{aligned} \quad (13)$$

$$C_{p_m}^\circ = -\frac{2}{\phi_m} \frac{J'_{\mu_m}(k_1 c)}{\Delta_{\mu_m}} \frac{k_2}{k_1} \sum_{n=-\infty}^{\infty} D_n^\circ F'_n(k_2 b) f_{n\mu}^m + \frac{2}{\phi_m} \frac{J'_{\mu_m}(k_1 b)}{\Delta_{\mu_m}} \frac{k_o}{k_1} \sum_{n=-\infty}^{\infty} \left\{ s_n H_n^{(2)}(k_o \rho_i) J'_n(k_o c) + A_n^\circ H_n^{(2)'}(k_o c) \right\} f_{n\mu}^m \quad (14)$$

$$s_k H_k^{(2)}(k_o \rho_i) J_k(k_o c) + A_k^\circ H_k^{(2)'}(k_o c) = \sum_{m=1}^N \sum_{n=-\infty}^{\infty} D_n^\circ F'_n(k_2 b) M_{nk}^m + \sum_{m=1}^N \sum_{n=-\infty}^{\infty} \left\{ s_n H_n^{(2)}(k_o \rho_i) J'_n(k_o c) + A_n^\circ H_n^{(2)'}(k_o c) \right\} Q_{nk}^m \quad (15)$$

$$D_k^\circ F_k(k_2 b) = \sum_{m=1}^N \sum_{n=-\infty}^{\infty} D_n^\circ F'_n(k_2 b) I_{nk}^m + \sum_{m=1}^N \sum_{n=-\infty}^{\infty} \left\{ s_n H_n^{(2)}(k_o \rho_i) J'_n(k_o c) + A_n^\circ H_n^{(2)'}(k_o c) \right\} R_{nk}^m \quad (16)$$

The above simultaneous equation can be rewritten in the following matrix form

$$\begin{pmatrix} \Psi_1 & \Psi_2 \\ \Psi_3 & \Psi_4 \end{pmatrix} \begin{pmatrix} s_n H_n^{(2)}(k_o \rho_i) J'_n(k_o c) + A_n^\circ H_n^{(2)'}(k_o c) \\ D_n^\circ F_n(k_2 b) \end{pmatrix} = \begin{pmatrix} \Gamma \\ 0 \end{pmatrix} \quad (17)$$

where A_n and D_n are column vectors and Ψ_1 , Ψ_2 , Ψ_3 , Ψ_4 , and Γ are matrices whose elements are

$$\begin{aligned} \psi_{1,nk} &= \sum_{m=1}^N Q_{nk}^m - \frac{H_n^{(2)}(k_o c)}{H_n^{(2)'}(k_o c)} \delta_{nk} \\ \psi_{2,nk} &= \sum_{m=1}^N \frac{F'_n(k_2 b)}{F_n(k_2 b)} M_{nk}^m \\ \psi_{3,nk} &= - \sum_{m=1}^N R_{nk}^m \\ \psi_{4,nk} &= \delta_{nk} - \sum_{m=1}^N \frac{F'_n(k_2 b)}{F_n(k_2 b)} I_{nk}^m \\ \gamma_n &= - \frac{2j}{\pi k_o c} \frac{s_n H_n^{(2)}(k_o c)}{H_n^{(2)'}(k_o c)}. \end{aligned}$$

Solving the above matrices for A_n° and D_n° , we have

$$\begin{aligned} A_n^\circ H_n^{(2)'}(k_o c) &= (\Psi_1 - \Psi_2 \Psi_4^{-1} \Psi_3)^{-1} \Gamma - s_n H_n^{(2)}(k_o \rho_i) J'_n(k_o c) \\ D_n^\circ F_n(k_2 b) &= -\Psi_4^{-1} \Psi_3 (\Psi_1 - \Psi_2 \Psi_4^{-1} \Psi_3)^{-1} \Gamma. \end{aligned} \quad (18)$$

Once A_n° and D_n° are determined, the coefficient $B_{p_m}^\circ$ and $C_{p_m}^\circ$ can be found by using (13) and (14).

4. NUMERICAL RESULTS

In order to verify that the infinite series involved in the solution is rapidly convergent, the general example is considered. The example shows the variation of the backscattering echo width for two parallel strips of $b = 0.75\lambda_o$, $c = 1.25\lambda_o$ with the number of the infinite series, n . As one can see from Fig. 4 the convergence is achieved after $n = 15$ for a dimension of $2.5\lambda_o$. That is relatively a small number of terms required to achieve the convergence.

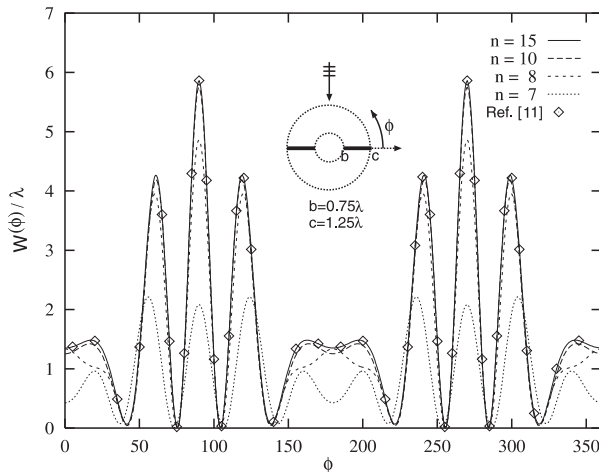


Figure 4. Backscattering echo width for two parallel strips of $b = 0.75\lambda_o$, $c = 1.25\lambda_o$ with the number of the infinite series number n .

Figure 5 shows the normalized backscattering (radar) cross section versus frequency (kb) of an uncoated multi-slotted cylinder. As observed in Figs. 5(a) and (b), when the wave hits the aperture directly, the effect of resonances makes the structure strongly frequency-dependent. Therefore, RCS dependence on the angle of orientation, even if they are close to each other, will be quite different as shown in Figs. 5(b) and (c).

Figure 6 represents the radiated field versus frequency through a slot in a thick circular shell with $\phi_1 = 60^\circ$. The slot is filled with air and the source is an electric line current at four different positions. When the source is at the center of the shell, the resonance peaks at 2.30 and 5.42 corresponding to the TM_{01} and TM_{02} modes while the

resonance nulls at 3.83, 5.13, 6.37 and 7.01 corresponding to the TM_{11} , TM_{21} , TM_{31} and TM_{12} modes. Fig. 6 shows that the frequencies of resonance nulls are varied by the positions of the electric line current.

In Fig. 7, the transmission and shielding effects due to different positions of the electric current are shown by comparing contour plots

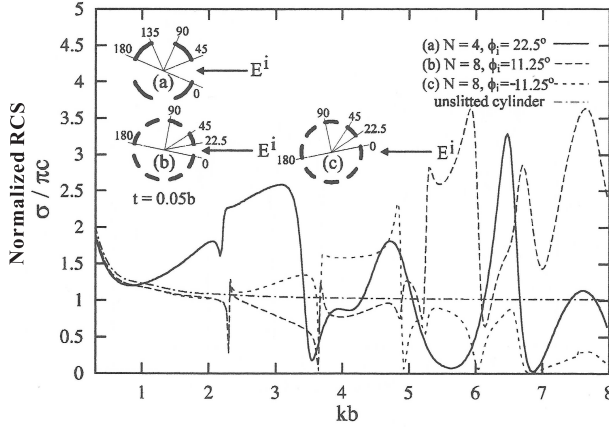


Figure 5. The normalized backscattering (radar) cross section versus frequency (kb) of an uncoated multi-slotted cylinder.

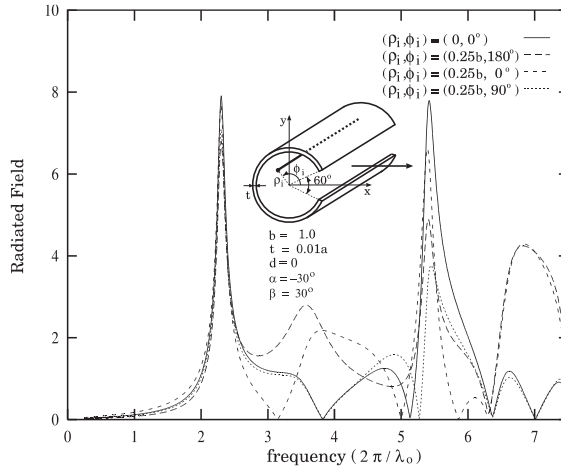


Figure 6. The radiated field versus frequency through a slotted circular cylinder with the electric line current at four different positions and $\phi_1 = 60^\circ$, $b = 1.0m$ and $t = 0.01b$.

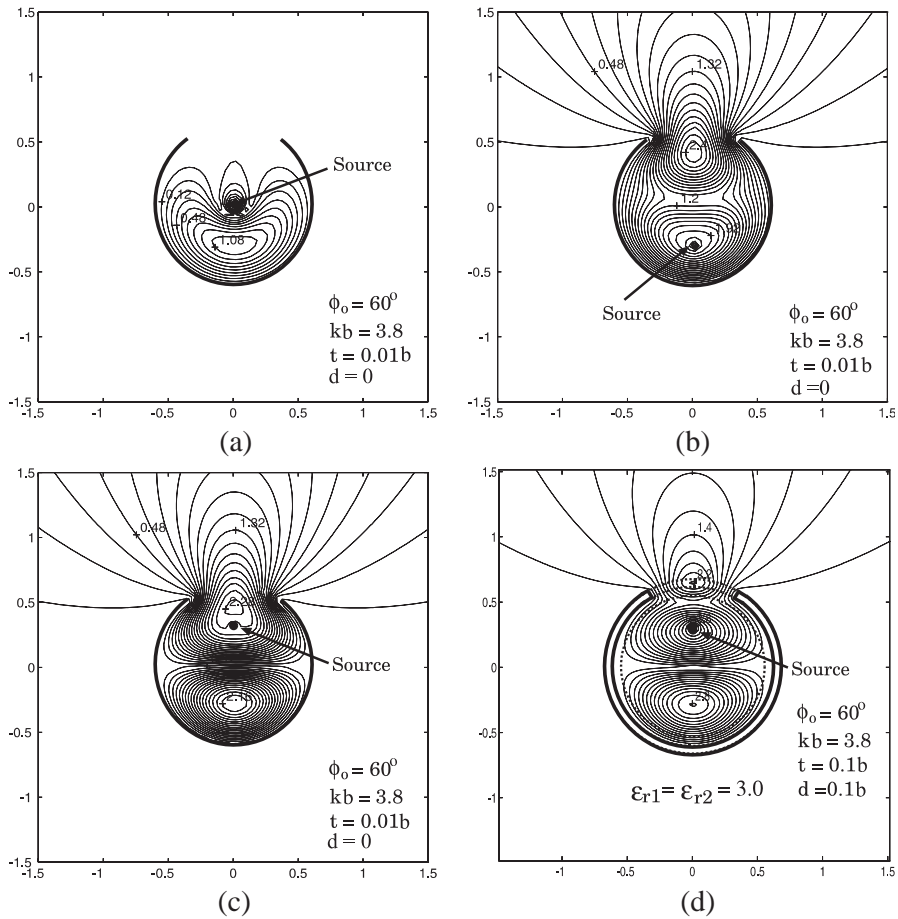


Figure 7. Contour plots of the electric field of a slotted circular cylinder with thickness with different positions of an electric current and $ka = 3.8$ and $\phi_o = 60^\circ$.

of the electric field with $ka = 3.8$ and $\phi_o = 60^\circ$. In Fig. 7(a), when the source is at the center of the shell, the field is not radiated from the aperture. In contrast, the field is excited with the TM_{11} mode and radiated from the aperture in Figs. 7(b) and (c). Fig. 7(d) shows the transmission and shielding effects of covering the aperture with dielectric ($\epsilon_{r2} = 3.0$, $t = 0.1b$) and coating the shell with dielectric ($\epsilon_{r1} = 3.0$, $d = 0.1b$). It is shown that new resonance peak occurs at the thick dielectric cover.

Figure 8 shows the far field radiated through a slot in a thick

circular shell. The effect of dielectric constant on the radiated field is plotted for two different dielectric thickness and aperture width of the slot. This figure suggests that the dielectric cover over the slot causes a resonance to take place as a function of ε_{r2} . For a thick dielectric, the first resonance effect is observed when ε_{r2} is about 2.3 at $\phi_1 = 30^\circ$. When the thickness of the dielectric is reduced from 0.2λ to 0.1λ , the first resonance occurs at a higher value of the dielectric constant. It is

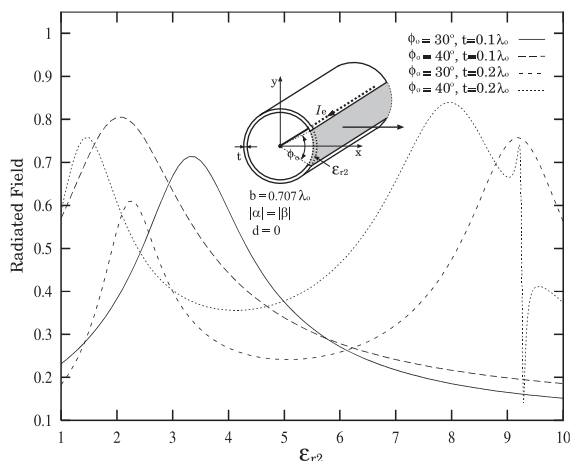


Figure 8. The radiated field versus ε_{r2} through a dielectric-filled slotted circular cylinder with an electric line current at the center of the shell.

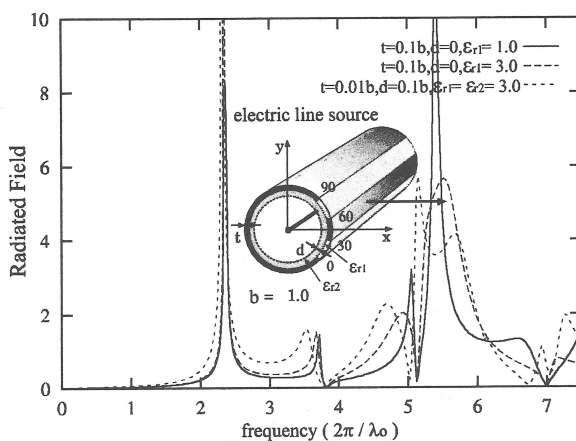


Figure 9. The radiated field versus frequency through the dielectric coated two-slotted cylinder ($\phi_1 = \phi_2 = 30^\circ$) with an electric line current at the center of the shell.

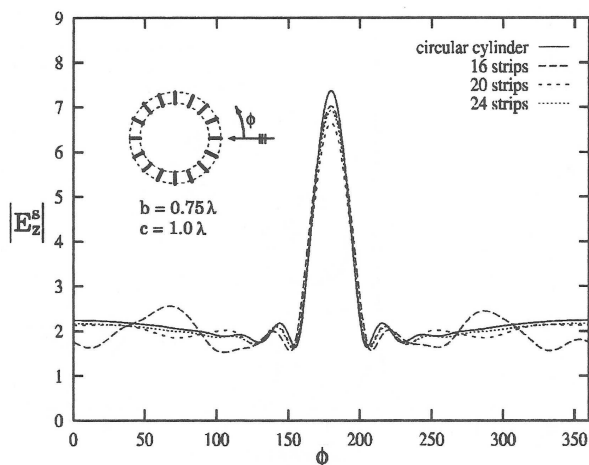


Figure 10. Far field patterns versus ϕ for multiple-strip circle located in a radial direction with respect to the center of cylinder.

also quite surprising to see such a larger dependence on ε_{r2} of energy radiated outside, especially for the thin dielectric case at 0.1λ .

Figure 9 shows the radiated field versus frequency through the dielectric coated two-slotted cylinder ($\phi_1 = \phi_2 = 30^\circ$) with an electric line current at the center of the shell. Fig. 10 shows the far field patterns versus ϕ for multiple strips located in a radial direction with respect to the center of cylinder.

5. CONCLUSION

The new formulation of scattering and shielding effect of the electric line current placed inside or outside the dielectric-filled multi-slotted cylinder with thickness was presented in this paper. The radial mode matching technique was used to obtain the radiated field in series form. Radiating and coupling properties for a thick-coated multi-slotted cylinder were given for several cases.

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